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(54) Carrier and symbol synchronisation for multicarrier signals

(57) A method and a corresponding apparatus are described for the time and frequency synchronization in transmission and reception systems with multi-carrier modulation of the OFDM type, as for instance the digital television system known as DVB-T and the digital audio system known as DAB. In particular the method refers to the correction of the residual frequency deviation Δf

and to the correction of the difference $1/\Delta T_o$ between the sampling frequencies of the transmitter and the receiver. The solution foresees the estimation of Δf and $1/\Delta T_o$ through the minimum square approximation, using only a single recursive algorithm with successive corrections.

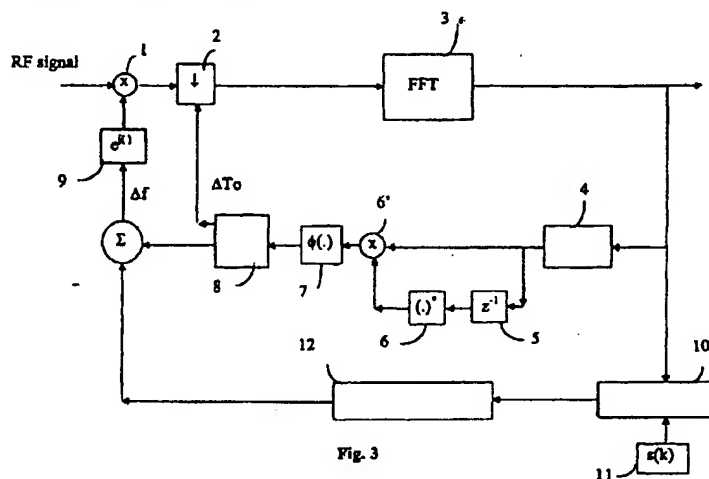


Fig. 3

Description

[0001] The present invention refers to a method and a corresponding apparatus for the time and frequency synchronization in transmission and reception systems with multi-carrier modulation of the OFDM (Orthogonal Frequency Division Multiplexing) type. DVB-T (Digital Video Broadcasting - Terrestrial) and DAB (Digital Audio Broadcasting) are based on this modulation type.

[0002] DVB-T is the European system for the terrestrial transmission of a digital television signal according to the specification "ETS 300 744, Framing structure channel coding and modulation for digital Terrestrial Television, March 1997". Said system provides two transmission modes called 2k and 8k, depending on the fact that the OFDM modulation has respectively 1705 or 6817 carriers, also called cells, modulated QPSK (Quadrature Phase Shift Keying), or 16 QAM (Quadrature Amplitude Modulation) or 64 QAM. The set of the values transmitted in one defined instant on the 1705 or 6817 carriers or cells is called OFDM symbol.

[0003] The DAB system for the transmission of the digital audio signal is based on the specification "ETS 300 401, Radio Broadcasting Systems; Digital Audio Broadcasting to mobile, portable and fixed receivers, January 1994", and provides three transmission modes which differ for the number of carriers used in the OFDM modulation. There are 1536 carriers in the mode 1, 384 in the mode 2 and 192 in the mode 3, therefore a symbol is made out of 1536, 384 or 192 carriers or cells. The carriers are modulated by using the system known as $\pi/4$ - shifted DQPSK (Differential Quadrature Phase Shift Keying), as shown in the publication "Digital Communications" by J.D. Proakis, Mc Graw-Hill International Editions.

[0004] In the said OFDM systems, as time synchronization we understand the alignment of the sampling frequency of the transmitter with that of the receiver, while the frequency synchronization provides for the correction of the frequency deviation introduced in reception in the base band translation of the signal transmitted in the pass-band. For the identification and the consequent removal of great part of the frequency deviation the known and proved solution which is used is the so-called "correlation solution", as described e.g. in the article "A Digital Audio Broadcasting (DAB) Receiver" by K. Taura, M. Tsujishita et al, IEEE Transactions on Consumer Electronics, vol. 42, no. 3, August 1996, pp. 322-327. By means of this technique particular, known to the receiver, pseudo-random sequences are transmitted, and they are characterized by having a quasi-impulsive auto-correlation. In this way, by performing a correlation between the received symbol and the known sequence it is possible in reception to estimate the frequency deviation, analyzing the shifting which is necessary for obtaining the maximum value of correlation. In fact such a maximum will be obtained in correspondence of the nearest integer to the normalized frequency deviation, which is the ratio between the frequency deviation and the sub-channel spacing, i.e. the spacing between two adjacent carriers.

[0005] With this method it is therefore possible to avoid a frequency deviation equal to one or more multiples of the sub-channel spacing.

[0006] The synchronization techniques have been the subject of several studies, particularly in the article "A technique for Orthogonal Frequency Division Multiplexing frequency offset correction", by P.H. Moose, IEEE Transactions on Communications, vol. 42, no. 10, October 1994, pp. 2908-2914, where an estimation technique has been proposed with the maximal probability of the frequency deviation. In the article "A frequency and timing acquisition technique for OFDM systems", by H. Nogami and T. Nagashima, Proceedings PMRC '95, vol. 3, pp. 1010-1015, a technique has been proposed for the simultaneous synchronization of the frequency deviation and the sampling frequency with a not efficient average value estimation of the errors. The said techniques have the disadvantage of completely neglecting the difference between the actual sampling frequencies in transmission and reception, or of estimating it in a not precise and not efficient manner.

[0007] Aim of the present invention is that of indicating an improved method, and an apparatus using said method, for obtaining a correction of both the residual frequency deviation Δf and the difference $1/\Delta T_0$ between the sampling frequencies; in particular said method uses only a single algorithm for the contemporary estimation of the errors, so that the control of the synchronization in reception is simplified.

[0008] For realizing such aim the present invention has as subject a method, and a corresponding apparatus, having the characteristics described in the attached claims, which are an integral part of the present description.

[0009] Further aims, characteristics and advantages of the present invention will be clear from the following detailed description and the attached drawings, supplied only as explanatory and non limiting examples, wherein:

- fig. 1 shows the structure of the transmitted DVB-T signal;
- fig. 2 shows the principle of the calculation on which the invention is based;
- fig. 3 shows the recursive pattern for the synchronization of a DVB-T signal with pilot cells of the continual type according to the invention;
- fig. 4 shows the time correction pattern for the pilot cells of the continual type;
- fig. 5 shows the time correction pattern for the pilot cells of the scattered type;
- fig. 6 shows the recursive pattern for the synchronization of a DAB signal according to the invention.

[0010] For making the reading easier the symbols and terms used in the following are listed below.

- FFT: Fast Fourier Transform
 IFFT: Inverse Fast Fourier Transform
 5 PRS: Phase Reference Symbol
 N: number of carriers
 p: current carrier index
 p_i: pilot carrier index
 DQPSK: Differential Quadrature Phase Shift Keying
 10 v: duration of the guard interval
 CPC: continual pilot cells
 SPC: scattered pilot cells
 P_{CPC}: set of the CPC carrier indexes
 P_{SPC}: set of the SPC carrier indexes
 15 ∈: symbol of belonging to a set
 F_o: channel speed
 F = F_o/N: sub-channel spacing
 T_o = 1/F_o: temporal quantum of the channel
 T = (N+v)T_o: symbol duration in transmission
 20 Δf: frequency deviation
 T'_o: temporal quantum in reception
 ΔT_o = T_o - T'_o: sampling interval deviation
 1/ΔT_o: deviation from the sampling frequency
 T' = (N+v)T'_o: symbol duration in reception
 25 Δf/F: normalized frequency deviation
 ΔT_o/T_o: normalized sampling frequency deviation
 X_p(nT): pth carrier, i.e. pth input of the IFFT modulation block at instant nT
 X'_p(nT): pth output of the IFFT demodulation block at instant nT

30 [0011] In the DVB-T system an OFDM symbol is constituted, as said, by a set of 1705 carriers (2k mode) or 6817 carriers (8k mode) which are contemporarily transmitted; the transmission is organized in frames composed by 68 symbols. Four consecutive frames build a "superframe". Each frame contains, besides cells or data carriers, also special cells, called pilot cells, which are used in reception for the synchronization of the OFDM signal, and are transmitted at a power level amplified by a factor 16/9 in respect of the normal cells carrying the data of the television signal. The pilot cells are of two types: "scattered", in the following called SPC cells, and "continual", in the following CPC cells, and transmit known data pertaining to a pseudo-random binary sequence (shortly PRBS).

35 [0012] Fig. 1 shows the position of the SPC cells in a frame; in the figure the vertical columns represent the succession of the symbols in a frame, while k indicates the position of a cell in a symbol, with 0 ≤ k ≤ k_{max}, where k_{max} is equal to 1704 or 6816. We can notice that the SPC cells appear in the same position every 4 symbols; the CPC cells, not shown in the figure, instead are repeated every symbol in the precise positions defined by the standard (positions 0, 48, 54, 87, 141, etc.). In other words the pilot cells have a repetition period equal to a multiple m of the period of the symbol: for the CPC cells m = 1, while for the SPC cells m = 4.

[0013] Taking in account the frequency deviation, the temporal deviation and the various distortions introduced, the relationship between the pth received carrier X'_p and the same transmitted carrier X_p is:

$$45 \quad X'_p(nT) = X_p(nT) H(pF) A_p e^{j(2\pi/N)(N+v)[n(p \Delta T_o/T_o - \Delta f/F) + \varphi_p]} \quad 1)$$

where φ_p , A_p e $H(pF)$ represent respectively a phase shift, an actual attenuation and the frequency response in base band of the channel at the frequency pF, while ΔT_o is the variation of the sampling interval and Δf is the residual frequency variation. Evaluating the 1) in two consecutive periods (n+1)T' and nT' for the CPC cells which, as said, occupy the same position in all symbols, we obtain the relationship:

$$50 \quad X'_p((n+1)T') X'_p(nT') = X_p((n+1)T) X_p(nT) |H(pF)|^2 A_p^2 e^{j(2\pi/N)(N+v)[p_1 \Delta T_o/T_o - \Delta f/F]} \text{ with } p_1 \in P_{CPC} \quad 2)$$

55 where the scientific notation * means conjugate complex.

[0014] The same relationship is valid for the SCP, but evaluating the 1) in the periods (n+4)T' and nT', as the SPC have a period of 4 symbols:

$$X'p_i((n+4)T) X'p_i^*(nT) = Xp_i((n+4)T) Xp_i^*(nT) |H(pF)|^2 A_p^2 e^{j(8\pi/N)(N+v)[p_i \Delta T_o/T_o - \Delta f/F]} \text{ with } p_i \in P_{SPC} \quad 3)$$

[0015] Relationships 2) and 3), where the symbols Xp_i are known and constant in time, constitute the basis of the invention; they can also be written:

$$p_i (\Delta T_o/T_o) - \Delta f/F = N/(2\pi(N+v)) \arg(X'p_i(n+1)T) X'p_i^*(nT)) , p_i \in P_{CPC} \quad 4)$$

$$p_i (\Delta T_o/T_o) - \Delta f/F = N/(8\pi(N+v)) \arg(X'p_i(n+4)T) X'p_i^*(nT)) , p_i \in P_{SPC} \quad 5)$$

and, by defining

$$\phi_{pi} = \arg(X'p_i((n+1)T) X'p_i^*(nT)) \text{ and } L = N/(2\pi(N+v)) \text{ for the CPC cells}$$

$$\phi_{pi} = \arg(X'p_i((n+4)T) X'p_i^*(nT)) \text{ and } L = N/(8\pi(N+v)) \text{ for the SPC cells}$$

we get

$$p_i (\Delta T_o/T_o) - \Delta f/F = L \phi_{pi} , p_i \in P_{CPC} \text{ or } p_i \in P_{SPC} \quad 4')$$

[0016] In the 4') p_i is the pilot carrier index and ϕ_{pi} the differential phase, i.e. the difference of phase of a pilot carrier in two adjacent symbols (P_{CPC} carrier) or in symbols spaced of 4 consecutive periods (P_{SPC} carrier).

[0017] For each carrier of the P_{CPC} or P_{SPC} set we can calculate couples of values $(p_o, \phi_{po}), (p_1, \phi_{p1}), (p_2, \phi_{p2}), \dots, (p_i, \phi_{pi}), \dots$ which, in the Cartesian plane (p, ϕ_p) represent points where the straight line defined by the 4') passes. It is to be noticed that ΔT_o and Δf vary from carrier to carrier.

[0018] The principle on which the invention is based provides the estimation of Δf , i.e. the residual deviation, and $1/\Delta T_o$, i.e. the sampling frequency deviation, by means of the straight line that approximates at best all the Cartesian points having coordinates (p_i, ϕ_{pi}) , with $p_i \in P_{CPC}$ or $p_i \in P_{SPC}$. Such straight line represents the desired estimations, as Δf is given, apart from the factor $1/LF$, by the intersection of that line and the axis of ordinates, while the angular coefficient $\tan \alpha$ of the line yields the estimation of ΔT_o , apart from the factor $1/LT_o$, as shown in fig. 2.

[0019] In mathematical terms, that line is determined by means of the known minimum squares approximation, according to which the desired for estimation is that which minimize the sum of the squares of the single errors; the desired estimations $\Delta \hat{T}_o$ and $\Delta \hat{f}$ are therefore those which minimize the quantity:

$$S = \sum_{i=0}^{N_p-1} \left[\phi_{pi} - \frac{1}{L} \left(\frac{\Delta \hat{T}_o}{T_o} p_i - \frac{\Delta \hat{f}}{F} \right) \right]^2 \quad 6)$$

where N_p is the number of the continual or scattered pilot carriers.

[0020] The originality of the proposed solution is in the possibility of estimating contemporarily and in a reliable manner ΔT_o and Δf so notably simplifying the operation of synchronizing while receiving.

[0021] Practically the synchronization with CPC carriers is made according to the recursive pattern of fig. 3, wherein the block number 1 converts in base band the radio frequency signal RF, the block 2 represents the sampling, the block 3 represents the FFT operation for reconstructing in reception the symbols, in the block 4 the CPC carriers are extracted, the block 5 inserts a delay equal to a period of a symbol, the block 6 performs the conjugate complex operation, the block 6' multiplies the signals coming from blocks 4 and 6, the block 7 calculates the ϕ_{pi} phases, in the block 8 the estimation is performed for the line which approximates at best the points (p, ϕ_p) , i.e. the values of ΔT_o and Δf are calculated which minimize the 6); the block 9 generates the frequency for the translation in base band performed by block 1. In the bottom part of fig. 3 the removal of most of the frequency deviation is performed by means of the already cited correlation method; the block 10 performs in fact the correlation between the received symbol and the sequence $s(k)$ generated in block 11 and which is defined by

$$s(k) = \begin{cases} \text{PRBS}(k) & \text{if } k \in P_{CPC} \\ 0 & \text{for other carriers} \end{cases}$$

[0022] The block 12, starting from the values delivered by the correlation, generates a first estimation of the frequency deviation, which is then perfected by means of the above described technique shown in the upper part of fig. 3.

[0023] It is important to notice that the described estimation technique generates the estimation starting from two consecutive symbols CPC, and it is therefore possible to estimate the deviations only every second symbol, as shown in the timing pattern of fig. 4.

[0024] For the solution with SPC cells the patterns are all equal to those of fig. 3 and 4 with the only changing of the time reference; actually in this case the delay produced by block 5 is of 4 symbols, while the estimation is obtained every 8 symbol periods, as shown in fig. 5.

[0025] The two synchronization techniques with CPC and SPC have different performances. By means of an analytic study and an accurate simulation, we demonstrated that the SPC solution gives a more precise estimation than the CPC solution, so that two synchronization levels are available, one fine with CPC and a second very fine with SPC.

[0026] The difference is due to the different characteristics of the sets of P_{CPC} and P_{SPC} carriers.

[0027] The P_{CPC} set is in fact composed by 45 carriers in the 2k mode and 177 carriers in the 8k mode, while the P_{SPC} set has 142 carriers in the 2k mode and 568 carriers in the 8k mode.

[0028] The greater number of carriers in the P_{SPC} solution allows a much better estimation of the minimum squares.

[0029] In the DAB system the transmission is organized in frames; each frame is constituted by the sequence of the null symbol, the PRS symbol (Phase Reference Symbol) and the symbols which contain the useful information, whose number varies according to the mode: 76 for modes 1 and 2, 153 for mode 3.

[0030] While for the synchronization of frame and the rough synchronization of frequency the said two symbols of every frame are used, by exploiting the auto-correlation property of PRS with a technique similar to that described for the DVB-T system, for the synchronization of the sampling frequency and the fine correlation of the frequency the useful data are adequately processed.

[0031] The analysis of the DAB system, in presence of frequency deviation and temporal deviation, yields the same results seen for the DVB-T system, as the two systems are analogous, so that the relation 1) between the received symbol and the transmitted symbol is still valid.

[0032] As, however, in the case of the DAB the pilot cells are missing, all the carriers of a symbol are used, carrying generally different and variable signals, because they represent, as said, the useful data. Relations 2), 4) and 4') are still valid, but they should be intended as extended to all carriers and not to the pilot carriers only.

[0033] As the standard provides the differential modulation $\pi/4$ - shift DQPSK, where the carriers phases are located at $\pi/4$, $3/4\pi$, $5/4\pi$ and $7/4\pi$, the contribution given in 2) by the data represents a phase equal to an odd multiple of $\pi/4$, which adds up to the phase associated to the errors. In order to solve the problem of the fine synchronization, the amount of errors and their phase are very small in comparison with a multiple of $\pi/4$, and therefore the latter can be easily isolated in the calculation.

[0034] The invention relating to the DVB-T system when applied to the DAB system provides for the estimation of Δf and ΔT_0 still using the straight line which at best approximates the points of coordinates (p, ϕ_p) , starting from the expression 4'), but where p takes all values comprised between 0 and $N-1$.

[0035] The 6) becomes therefore

$$S = \sum_{p=0}^{N-1} \left[\phi_p - \frac{1}{L} \left(\frac{\Delta \hat{T}_0}{T_0} p - \frac{\Delta \hat{f}}{F} \right) \right]^2 \quad 7)$$

where N is the total number of the carriers and $L = N/(2\pi(n+v))$.

[0036] Fig. 6 shows the recursive pattern for the DAB; block 7' eliminates the odd multiples of $\pi/4$ due, as said, to the modulation; block 11 represents the PRS generator. The other blocks have the same function of that of fig. 3, hence their description is not repeated here.

[0037] The advantages of the proposed method and the corresponding apparatus are now evident: firstly the estimation of Δf and $1/\Delta T_0$ is made by means of the minimum squares approximation using only one single recursive algorithm with successive approximations, and therefore in a very quick manner simplifying by far the control of the synchronization on the reception side; furthermore such estimation is made more reliable and efficient because it is based on the examination of samples received in two different symbols, i.e. on a greater number of pieces of information in comparison with the solutions that provide the estimation by examining samples of only one symbol.

[0038] It is clear that several variations can be made to the method and the apparatus according to the present invention without exiting from the scope of the novelty principles which are inherent to the inventive idea.

Claims

1. Method for the contemporary estimation of the error ($1/\Delta T_0$) between the sampling frequencies of a transmitter and a receiver and the residual frequency deviation (Δf) produced on the reception side, in a digital multi-carrier system of the OFDM type, characterized in that said estimation is obtained by means of the minimum squares approximation using only one single recursive algorithm with successive approximations.
2. Method for the contemporary estimation of the error ($1/\Delta T_0$) between the sampling frequencies of a transmitter and a receiver and the residual frequency deviation (Δf) according to claim 1, characterized in that for said estimation the carriers are used which are received in two different symbols.
3. Method for the contemporary estimation of the error ($1/\Delta T_0$) between the sampling frequencies of a transmitter and a receiver and the residual frequency deviation (Δf) according to claim 2, characterized in that the carriers are constituted by the pilot carriers.
4. Method for the contemporary estimation of the error ($1/\Delta T_0$) between the sampling frequencies of a transmitter and a receiver and the residual frequency deviation (Δf) according to claim 3, characterized in that the carriers are of the scattered type.
5. Method for the contemporary estimation of the error ($1/\Delta T_0$) between the sampling frequencies of a transmitter and a receiver and the residual frequency deviation (Δf) according to claim 3, characterized in that the carriers are of the continual type.
6. Method for the contemporary estimation of the error ($1/\Delta T_0$) between the sampling frequencies of a transmitter and a receiver and the residual frequency deviation (Δf) according to claim 1, characterized in that the multi-carrier OFDM system is the television system known as DVB-T (Digital Video Broadcasting -Terrestrial).
7. Method for the contemporary estimation of the error ($1/\Delta T_0$) between the sampling frequencies of a transmitter and a receiver and the residual frequency deviation (Δf) according to claim 1, characterized in that the multi-carrier OFDM system is the digital radio broadcasting system known as Digital Audio Broadcasting (DAB).
8. Method for the contemporary estimation of the error ($1/\Delta T_0$) between the sampling frequencies of a transmitter and a receiver and the residual frequency deviation (Δf) according to claim 2, characterized in that the different symbols are temporal consecutive symbols.
9. Method for the contemporary estimation of the error ($1/\Delta T_0$) between the sampling frequencies of a transmitter and a receiver and the residual frequency deviation (Δf) produced on the reception side, in a digital multi-carrier system of the OFDM type, comprising one or more pilot carriers having a repetition period equal to a multiple m of the period of the symbol, m being an integer number, characterized by the following steps:
 - calculation of the differential phases $\phi_{pi} = \arg(X'p_i((n+m)T) X'p_i^*(nT))$, where $X'p_i(nT)$ and $X'p_i((n+m)T)$ are the symbols on the reception side of the pilot carrier in the periods of symbol nT and $(n+m)T$ and $X'p_i^*(nT)$ is the conjugate complex of $X'p_i(nT)$, of all the pilot carriers;
 - contemporary calculation of the estimated values of the residual frequency deviation $\Delta \hat{f}$ and of the sampling frequency deviation $1/\Delta \hat{T}_0$ which minimize the quantity

$$S = \sum_{i=0}^{N_p-1} \left[\phi_{pi} - \frac{1}{L} \left(\frac{\Delta \hat{T}_0}{T_0} p_i - \frac{\Delta \hat{f}}{F} \right) \right]^2$$

where N_p is the number of the pilot carriers and $L = N_p/2\pi m(N_p + v)$.

10. Method for the contemporary estimation of the error ($1/\Delta T_0$) between the sampling frequencies of a transmitter and a receiver and the residual frequency deviation (Δf) according to claim 9, characterized in that the OFDM multi-carrier system is the television system known as DVB-T (Digital Video Broadcasting -Terrestrial).

11. Method for the contemporary estimation of the error ($1/\Delta T_0$) between the sampling frequencies of a transmitter and a receiver and the residual frequency deviation (Δf) according to claim 10, characterized in that the pilot carriers have a repetition period equal to one symbol period, i.e. $m = 1$.
12. Method for the contemporary estimation of the error ($1/\Delta T_0$) between the sampling frequencies of a transmitter and a receiver and the residual frequency deviation (Δf) according to claim 10, characterized in that the pilot carriers have a repetition period equal to 4 symbol periods, i.e. $m = 4$.
13. Method for the contemporary estimation of the error ($1/\Delta T_0$) between the sampling frequencies of a transmitter and a receiver and the residual frequency deviation (Δf) produced on the reception side, in a digital multi-carrier system of the OFDM type, comprising N carriers, each one with differential modulation $\pi/4$ - shifted Differential Quadrature Phase Shift Keying (DQPSK), characterized by the following steps:
- calculation of the differential phases $\phi_p = \arg(X'p((n+1)T) X'p^*(nT))$, where $X'p(nT)$ and $X'p((n+1)T)$ are the symbols on the reception side of the p^{th} carrier in the periods of symbol nT and $(n+1)T$ and $X'p^*(nT)$ is the conjugate complex of $X'p(nT)$, of all the carriers;
 - removal from each ϕ_p of a quantity equal to $n\pi/4$, where n is an odd integer so that $n\pi/4 < |\phi_p| < (n+2)\pi/4$;
 - contemporary calculation of the estimated values of the residual frequency deviation $\Delta \hat{f}$ and of the sampling frequency deviation $1/\Delta \hat{T}_0$ which minimize the quantity

$$S = \sum_{p=0}^{N-1} \left[\phi_p - \frac{1}{L} \left(\frac{\Delta \hat{T}_0}{T_0} p - \frac{\Delta \hat{f}}{F} \right) \right]^2$$

where N is the number of the carriers and $L = N/2\pi(N + v)$.

14. Method for the contemporary estimation of the error ($1/\Delta T_0$) between the sampling frequencies of a transmitter and a receiver and the residual frequency deviation (Δf), according to claim 13, characterized in that the OFDM system is the digital radio broadcasting system known as Digital Audio Broadcasting (DAB).
15. Apparatus for the contemporary estimation of the error ($1/\Delta T_0$) between the sampling frequencies of a transmitter and a receiver and the residual frequency deviation (Δf) produced on the reception side, in a digital multi-carrier system of the OFDM type, comprising one or more pilot carriers having a repetition period equal to a multiple m of the period of the symbol, m being an integer number, characterized in that it comprises means (4) for extracting the symbols $X_{p_i}(nT)$ of the pilot carriers p_i , means (5) for delaying said symbols of said carriers of m symbol periods, means (6) for performing the conjugate complex operation on said delayed symbols, means (6') for multiplying the non delayed symbols and the conjugate complexes of the delayed symbols, means (7) for obtaining the differential phases $\phi_{p_i} = \arg(X'p_i((n+m)T) X'p_i^*(nT))$, and means (8) for the contemporary estimation of the values $\Delta \hat{f}$ and $1/\Delta \hat{T}_0$ which minimize the quantity

$$S = \sum_{i=0}^{N_p-1} \left[\phi_{p_i} - \frac{1}{L} \left(\frac{\Delta \hat{T}_0}{T_0} p_i - \frac{\Delta \hat{f}}{F} \right) \right]^2$$

where N_p is the number of the pilot carriers and $L = N_p/2\pi m(N_p + v)$.

16. Apparatus for the contemporary estimation of the error ($1/\Delta T_0$) between the sampling frequencies of a transmitter and a receiver and the residual frequency deviation (Δf) produced on the reception side, in a digital multi-carrier system of the OFDM type, characterized in that it uses a method according to one or more of the preceding claims.
17. Apparatus for the contemporary estimation of the error ($1/\Delta T_0$) between the sampling frequencies of a transmitter and a receiver and the residual frequency deviation (Δf) produced on the reception side, in a digital multi-carrier system of the OFDM type, characterized in that it comprises means (5) for delaying the symbols of the carriers of

one symbol period, means (6) for performing the conjugate complex operation on said delayed symbols, means (6') for multiplying the non delayed symbols and the conjugate complexes of the delayed symbols, means (7) for obtaining the differential phases $\phi_p = \arg(X'_p((n+1)T) X'^*_p(nT))$, means (7') for removing from each ϕ_p a quantity equal to $n\pi/4$, where n is an odd integer so that $n\pi/4 < |\phi_p| < (n+2)\pi/4$, and means (8) for the contemporary estimation of the values $\Delta \hat{f}$ and $1/\Delta \hat{T}_0$ which minimize the quantity

$$S = \sum_{p=0}^{N-1} \left[\phi_p - \frac{1}{L} \left(\frac{\Delta \hat{T}_0}{T_0} P - \frac{\Delta \hat{f}}{F} \right) \right]^2$$

where N is the number of the carriers and $L = N/2\pi(N + v)$.

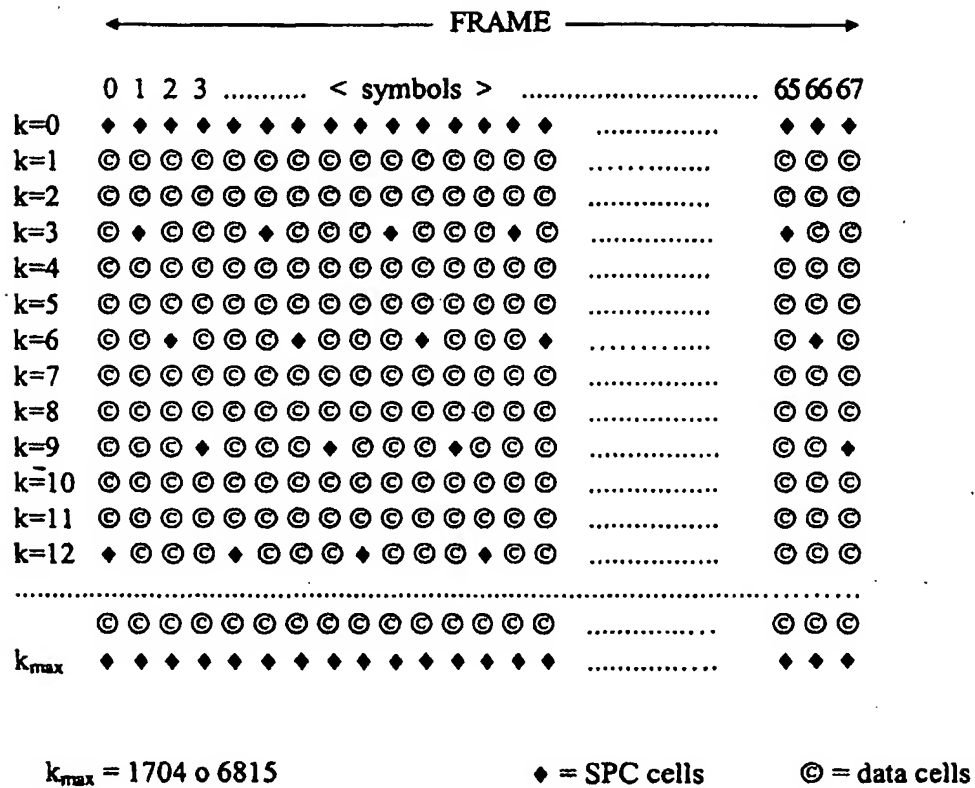
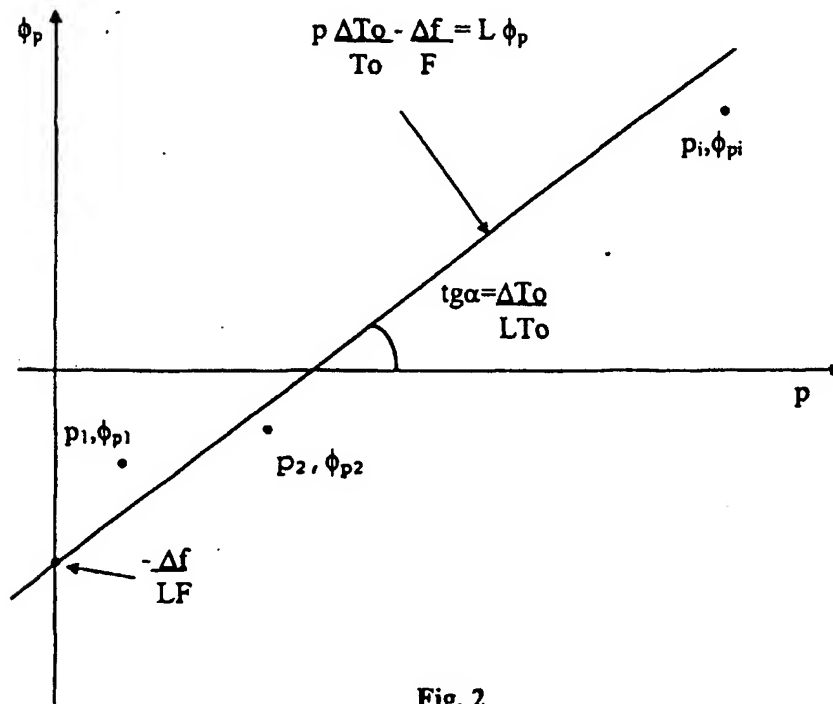
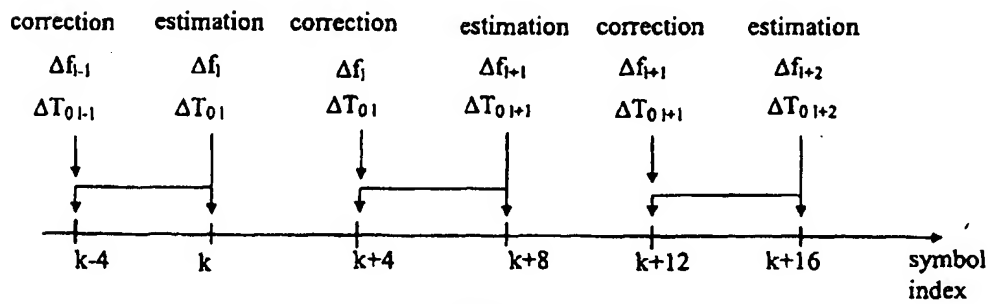
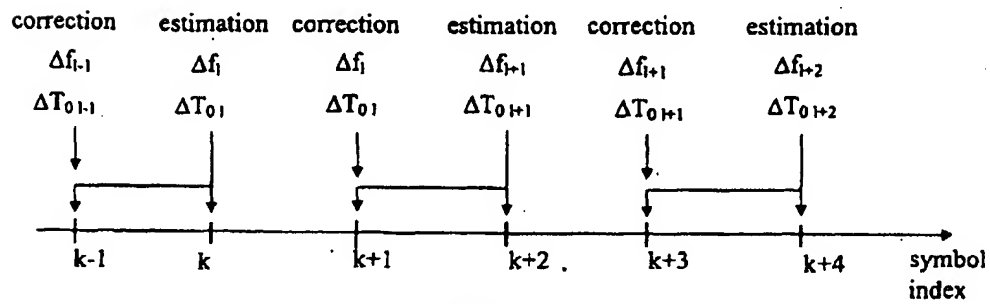
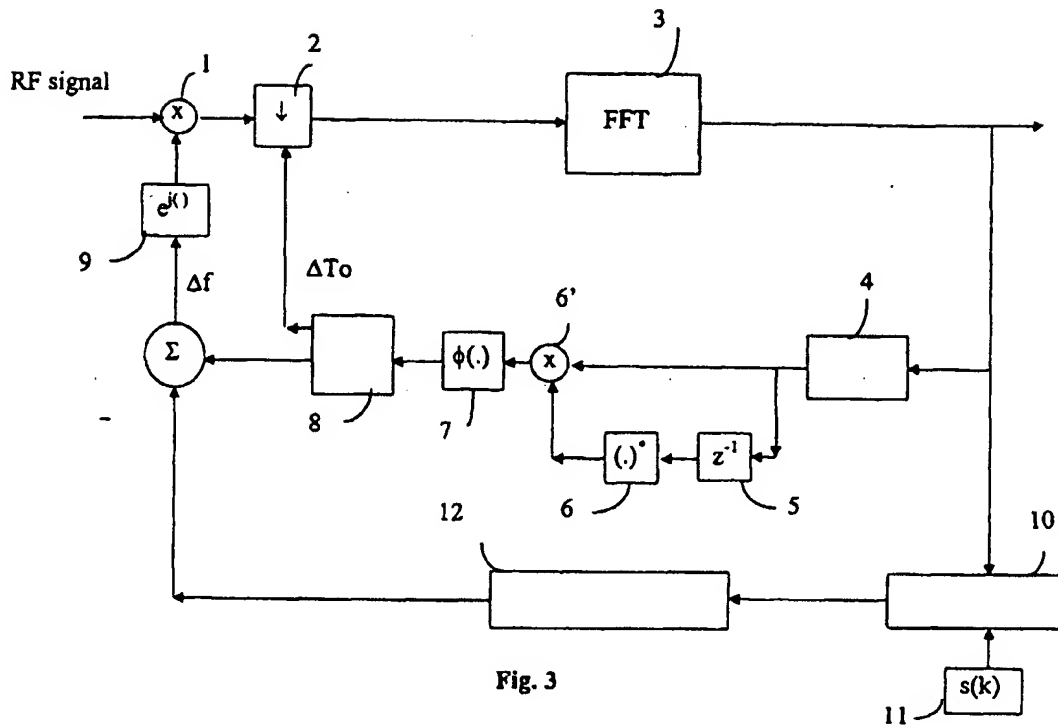


Fig. 1





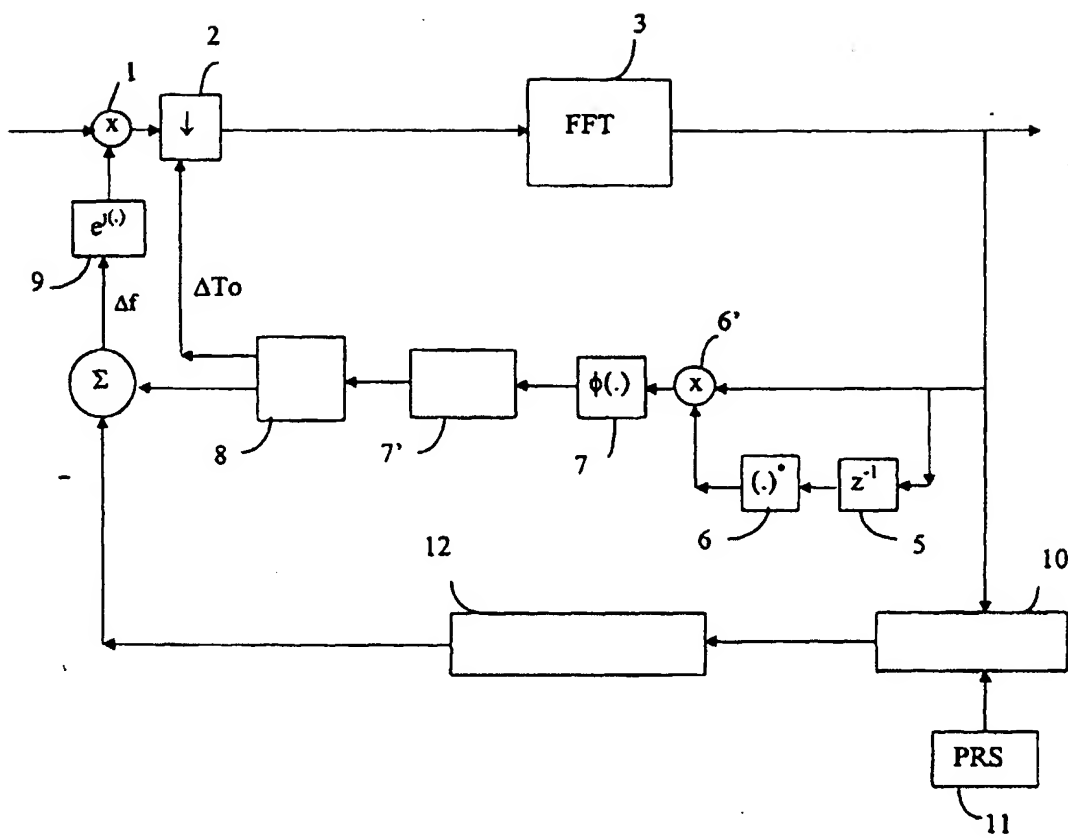


Fig. 6